

# Unitary Space-Time Modulation via the Cayley Transform

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**Abstract** — A method of generating good performing USTM constellations using the Cayley transform is proposed. The codes, which can be used for any number of transmit and receive antennas without channel knowledge, are designed based on an information-theoretic criterion, and lend themselves to polynomial-time near-maximum-likelihood decoding using the sphere decoding algorithm.

## I. INTRODUCTION

Consider a wireless communication system with  $M$  transmit antennas,  $N$  receive antennas and coherent interval  $T$ . A scheme called USTM that works without channel knowledge was proposed in [1], in which the transmitted signal  $S$  forms a unitary matrix. Further information-theoretic calculations [2] show that at high SNR, USTM can achieve channel capacity. In this paper, we propose to use the Cayley transform to design USTM constellations based on an information-theoretic criterion. The code is not only suitable for any number of  $M$  and  $N$ , but also has polynomial decoding complexity.

## II. CAYLEY USTM CODES

The Cayley transform of a complex  $T \times T$  matrix  $Y$  is defined to be  $V = (I + Y)^{-1}(I - Y)$  which provides a one-to-one map from the linear space of skew-Hermitian matrices to the nonlinear Stiefel manifold. So, it is convenient to encode data linearly onto a skew-Hermitian matrix and then apply the Cayley transform to get a unitary matrix. In [3], a class of *Cayley codes* for *differential* USTM was proposed. We extend it to the non-square case by choosing our  $S$  to be the first  $M$  columns of  $V$ . Let  $Y = iA$ , by adding structure on the Hermitian matrix  $A$  to *linearize* the near-ML decoder, our USTM codes can be written as  $S = [I_M + 2B\Delta_2^{-1}B^* \quad -2i\Delta_2^{-1}B^*]^T$  where  $\Delta_2 = I_{T-M} + B^*B - B^*A_{11}B + iA_{22}$ .  $A_{11} = \sum_{q=1}^{Q_1} \alpha_q A_{11,q}$ ,  $A_{22} = \sum_{p=1}^{Q_2} \beta_p A_{22,p}$  are upper-left  $M \times M$  and lower-right  $(T-M) \times (T-M)$  blocks of  $A$ .  $Q_1 + Q_2 = Q$  and  $B$  is some fixed  $M \times (T-M)$  matrix.  $\alpha_q$  and  $\beta_p$  are real scalars chosen from some set  $\mathcal{A}$  with cardinality  $r$  and carry the information. The  $A_{11,q}, A_{22,p}$  are fixed basis matrices. The transmit rate is clearly  $(Q/T) \log_2 r$ .

By ignoring the covariance of the additive noise term, the ML decoder can be reduced to some formula that is quadratic in  $\{\alpha_q\}$  and  $\{\beta_p\}$ . Setting the number of unknowns  $Q$  less than or equal to the number of independent linear equations [3], which is  $2N(T-M) - N^2$  for  $T-M \geq N$  and  $(T-M)^2$  for  $T-M < N$ , the decoding can be done in roughly  $O(Q^3)$  computations by sphere decoding.

From the information-theoretic analysis in [2, 3], the optimal distribution for  $V$  is an *isotropically-random* unitary matrix, which implies that  $A$  has the matrix Cauchy distribution. Drawing upon the implications from  $M = 1$  case, we choose

the set  $\mathcal{A}_r$  as the  $r$ -point discretization of a scalar Cauchy random variable.

Finally, we generalize the approach of [3] and use the criterion  $\max_{\{A_{11,q}\}, \{A_{22,p}\}, B} E \log \det(S^\perp - S^{\perp'})^*(S^\perp - S^{\perp'})$  to choose the basis matrices  $A_{11,q}, A_{22,p}$  as well as  $B$ , where the expectation is over  $\alpha_q$  and  $\beta_p$ . This optimization may be performed numerically using gradient-ascent methods along with Monte Carlo simulation.

## III. SIMULATION RESULTS

Fig.1 shows that there is little penalty (only around 1db) incurred when using the linearized ML instead of the true ML. In fig.2 we show that our method gains better performance than training scheme at high SNR even with a higher rate.

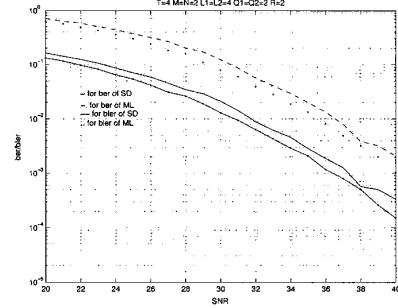


Fig 1: BER and BLER of linearized ML compared to the true ML.

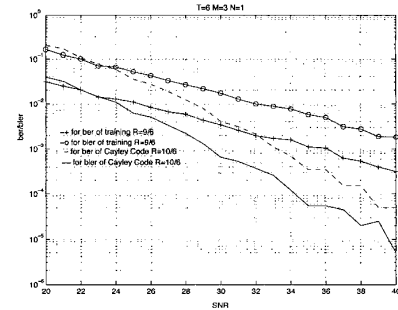


Fig 2: Cayley codes compared to training scheme.

## REFERENCES

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